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Fuzzy Static Output Feedback Control for Path Following of Autonomous Vehicles with Transient Performance Improvements

Anh-Tu Nguyen*, *Member, IEEE*, Chouki Sentouh, *Member, IEEE*, Hui Zhang, *Senior Member, IEEE*, and Jean-Christophe Popieul

Abstract—This paper provides a new solution for path following control of autonomous ground vehicles. \mathcal{H}_2 control problem is considered to attenuate the effect of the road curvature disturbance. To this end, we formulate a standard model from the road-vehicle dynamics, the *a priori* knowledge on the road curvature, and the path following specifications. This standard model is then represented in a Takagi-Sugeno fuzzy form to deal with the time-varying nature of the vehicle speed. Based on a static output feedback scheme, the proposed method allows avoiding expensive vehicle sensors while keeping the simplest control structure for real-time implementation. The concept of \mathcal{D} -stability is exploited using Lyapunov stability arguments to improve the transient behaviors of the closed-loop vehicle system. In particular, the physical upper and lower bounds of the vehicle acceleration are explicitly considered in the design procedure via a parameter-dependent Lyapunov function to reduce drastically the design conservatism. The proposed \mathcal{H}_2 design conditions are expressed in terms of linear matrix inequalities (LMIs) with a single line search parameter. The effectiveness of the new path following control method is clearly demonstrated with both theoretical illustrations and hardware experiments under real-world driving situations.

Index Terms—Autonomous vehicles, path following, vehicle dynamics control, fuzzy static output feedback control, \mathcal{D} -stability.

I. INTRODUCTION

Autonomous ground vehicles have become a major focus of today's automotive industry and academia [1], [2]. This has been motivated by two factors. First, over the years traffic statistics have shown a raising number of fatal road accidents, of which an estimation of 94% are caused by driver errors [3]. Second, recent advances in sensing technology, data processing and telecommunication enable the developments of driverless driving technology [1]. Apart from reducing dramatically the human driver's mistakes, autonomous vehicles provide a great freedom for everyday travels, especially for people with physical or visual disability.

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This paper is concerned with the path following control of autonomous ground vehicles. This typical motion control issue aims at designing steering control laws to reach and follow a desired path without a specific temporal specification [4]. Path following control for autonomous vehicles has received increasing attention, see [3], [5]–[10] and references therein. Using two independent PID nested loops, a vision-based lane keeping controller with successful experimental validation on roads with unknown curvature is proposed in [11]. A recent survey with a special focus on motion planning and feedback control of self-driving urban vehicles is presented in [3], in which a selection of control techniques are discussed, *e.g.*, pure pursuit, feedback linearization, control Lyapunov design, model predictive control (MPC). The authors in [12] provide an interesting analysis to highlight the advantages and drawbacks of three lateral controllers based on sliding mode control, immersion and invariance principle, and system passivity property. Another prominent comparative study between three controllers, including PID, linear-quadratic-Gaussian, and \mathcal{H}_∞ , on their performance limits and tradeoffs (in terms of lane tracking, stability robustness, and passenger comfort) is recently presented in [13]. In addition, obstacle-avoidance control is of crucial importance for autonomous vehicles. A two-stage nonlinear nonconvex control approach, consisting of an outer-loop nonlinear MPC and an inner-loop linear feedback control, is developed for obstacle avoidance in [14]. The authors in [15] develop a combined longitudinal-lateral control strategy for automated vehicle guidance where a nonlinear MPC technique is used for lateral control and the longitudinal speed tracking is guaranteed by another Lyapunov-based control law. Note that various other MPC-based control schemes have been applied to the path following and obstacle avoidance of autonomous vehicles [5], [16]–[18]. However, MPC technique requires solving online optimizations which leads to heavy computational burden, especially for nonlinear MPC problems as highlighted in [16]. Moreover, most of available results on vehicle path following control require *full* state-information for feedback designs. However, due to the excessive cost of vehicle sensors, the measurements of some vehicle states are not available on series-production vehicles, for instance the lateral speed and/or the sideslip angle [19], [20]. In this practical situation, an output feedback control scheme must be used [21]–[23]. It is stressed that output feedback MPC scheme is still an open-ended issue for which a moving horizon estimation must be considered [24].

For engineering applications, the transient behaviors of the closed-loop systems should be carefully studied since stability property is generally not sufficient for practical performance. It is well known that the closed-loop transient response of a linear system is related to the location of its poles. This fact was generalized to LMI (or \mathcal{D} -stability) regions for \mathcal{H}_∞ control design in [25]. The effectiveness of the \mathcal{D} -stability concept to improve the closed-loop transient response has been proved through a large range of control engineering systems, e.g., lateral vehicle dynamics [7], Diesel engine aftertreatment systems [26], etc. Despite numerous successful real-world applications, only few results on \mathcal{D} -stability for vehicle path following control are available, especially when using output feedback control schemes.

Motivated by the above theoretical and practical issues, we propose a novel robust \mathcal{H}_2 static output feedback (SOF) control scheme for path following of autonomous vehicles. In particular, this \mathcal{H}_2 control design fully exploits the \mathcal{D} -stability concept to improve the transient performance of the closed-loop vehicle system, thus the comfort of passengers. Note that the design of SOF controllers using \mathcal{D} -stability is NP-hard [27], and still widely open in the literature. Indeed, most of control applications, especially in intelligent automotive systems, are based on dynamic output feedback schemes [28]–[30]. Such a control scheme may induce complexity/difficulty in real-time implementation. To overcome this drawback, SOF control approaches were also proposed for vehicle path following in [4], [31], in which \mathcal{D} -stability was not considered. Note that the effects of the road curvature was not appropriately taken into account via the \mathcal{H}_2 SOF control design in [31]. Moreover, it may be hard to achieve *practically* a desirable path following performance with the approach in [4] due to the use of a genetic algorithm for the design procedure and the excessive number of linear submodels of the vehicle polytopic system. The contributions of this paper are summarized below.

- 1) Takagi-Sugeno (T-S) fuzzy control technique [32], [33] is exploited to take into account the *time-varying* nature of the vehicle speed. The physical bounds of the speed and the acceleration are explicitly considered in the control design to reduce the conservatism.
- 2) The proposed fuzzy SOF control method allows achieving practical performance on both: (1) closed-loop transient response to improve the passengers' comfort via \mathcal{D} -stability concept, and (2) vehicle path following under unknown road curvatures via a new \mathcal{H}_2 design based on a conceptual T-S fuzzy *standard model*. Using Lyapunov stability arguments, the \mathcal{H}_2 control design is reformulated as an LMI-based optimization problem, efficiently solved with convex semidefinite programming [34]. The proposed SOF control framework can be also applied to a large class of real-world applications.
- 3) The obtained control results are both *theoretically* and *practically* verified with relevant illustrations. To the best of our knowledge, experimental validations of \mathcal{H}_2 T-S fuzzy SOF control for path following of autonomous vehicles have not been reported in the open literature.

The paper is organized as follows. Section II presents the

vehicle nonlinear dynamics and defines the control goals. In Section III, a standard model is formulated for \mathcal{H}_2 control design. Using the \mathcal{D} -stability concept, Section IV discusses the new \mathcal{H}_2 SOF control design for T-S fuzzy systems which is applied later to the path following control. Section V provides experimental results to show the interests of the proposed method. Concluding remarks are drawn in Section VI.

Notation: Ω_N denotes the set $\{1, 2, \dots, N\}$. \mathbb{R} (respectively \mathbb{C}) is the field of real (respectively complex) numbers. I denotes the identity matrix of appropriate dimension. For a matrix X , X^\top indicates its transpose. For any square matrix X , $X \succ 0$ indicates a positive definite matrix, and $\text{He}X = X + X^\top$. $\text{diag}(X_1, X_2)$ denotes a block-diagonal matrix composed of X_1, X_2 . The symbol \star stands for matrix blocks that can be deduced by symmetry. \otimes denotes the Kronecker product of matrices. The argument of a function is omitted when its meaning is clear.

II. VEHICLE MODELING AND PROBLEM STATEMENT

This section reviews the vehicle modeling for lateral control purposes. The vehicle notation is given in Table I.

TABLE I
VEHICLE PARAMETERS

Notation	Description
M	Vehicle mass [kg]
l_f	Distance from the GC to front axle [m]
l_r	Distance from the GC to rear axle [m]
l_w	Distance from GC to wind impact point [m]
l_s	Look-ahead distance [m]
η_t	Tire length contact [m]
I_z	Inertia of vehicle yaw moment [kgm ²]
C_f	Front cornering stiffness [N/rad]
C_r	Rear cornering stiffness [N/rad]
f_w	Lateral wind force [N]
v_x	Vehicle longitudinal speed [m/s]
v_y	Vehicle lateral speed [m/s]
r	Vehicle yaw rate [rad/s]
δ	Vehicle steering angle [rad]

A. Nonlinear Vehicle Dynamics

A nonlinear single track model is used to represent the vehicle motions, see Fig. 1. This model captures the essential vehicle dynamics which is described as follows [11], [35]:

$$\begin{aligned} M(\dot{v}_x - rv_y) &= F_{xf} \cos \delta - F_{yf} \sin \delta + F_{xr} \\ M(\dot{v}_y + rv_x) &= F_{xf} \sin \delta + F_{yf} \cos \delta + F_{yr} + f_w \\ I_z \dot{r} &= l_f (F_{xf} \sin \delta + F_{yf} \cos \delta) - l_r F_{yr} + l_w f_w. \end{aligned} \quad (1)$$

The front/rear longitudinal forces F_{xi} and lateral forces F_{yi} are modeled using the following Pacejka's formula [36]:

$$\begin{aligned} F_{ki}(\alpha_i) &= D_i \sin(C_i \arctan \xi_i) \\ \xi_i &= (1 - E_i) B_i \alpha_i + E_i \arctan(B_i \alpha_i) \end{aligned}$$

where $k \in \{x, y\}$ and $i \in \{f, r\}$. The Pacejka parameters B_i , C_i , D_i and E_i depend on the characteristics of the tire, the road and the vehicle operating conditions. The sideslip angles of the front and rear tires are given by

$$\alpha_f = \delta - \arctan\left(\frac{v_y + l_f r}{v_x}\right), \quad \alpha_r = \arctan\left(\frac{l_r r - v_y}{v_x}\right).$$

where $\mathbf{x}_w = \rho_r$, $A_w = -\frac{1}{\tau_r}$, $B_w = -\frac{1}{\tau_r}$ and $C_w = 1$. The disturbance δ_w is an irreducible signal such as impulse or white noise [38].

Remark 1. Note that the model (5) does not allow for an accurate prediction of a curved trajectory. However, this *predictor* model provides *a priori* information on the dynamics of the road curvature, *i.e.*, via the time constant $\tau_r = 1$ [s]. This latter is reasonable for the prediction of the road curvature in most real-world driving situations. Then, the designed controller can exploit this information to predict and anticipate the system evolution to improve the overall closed-loop behaviors [38], [39]. The model Σ_w can be considered as an input shaping filter. This forbids *discontinuity* corresponding to the assumption that the road is composed of straight segments, circle arcs and clothoids [40]. In particular, for the case of autonomous driving, the introduction of ρ_r in the output \mathbf{y}_w of Σ_w allows incorporating a feedforward control action to improve the path following performance, especially when taking tight curves.

B. Control Performance Specifications

As can be seen later, the upper bound of the closed-loop \mathcal{H}_2 norm should be minimized to improve the control performance. To this end, the performance vector \mathbf{z} should involve variables correlated with the risk of lane departure (*e.g.*, heading error ψ_L and lateral deviation y_L), the driving comfort (*e.g.*, lateral acceleration $a_y \simeq v_x \dot{\beta}$), the energy consumption of the steering system and the comfort of passengers in terms of acceptability (*e.g.*, steering control angle δ), see [37]. Then, the performance vector \mathbf{z} is defined as

$$\mathbf{z} = \mathcal{W} \begin{bmatrix} \psi_L & y_L & a_y \end{bmatrix}^\top, \quad \mathcal{W} = \text{diag}(\omega_{\psi_L}, \omega_{y_L}, \omega_{a_y}),$$

where ω_{ψ_L} , ω_{y_L} , ω_{a_y} are the weighting coefficients and

$$\begin{bmatrix} \psi_L \\ y_L \\ a_y \end{bmatrix} = \begin{bmatrix} 0 & 0 & 1 & 0 \\ 0 & 0 & 0 & 1 \\ v_x a_{11} & v_x a_{12} & 0 & 0 \end{bmatrix} \mathbf{x}_p + \begin{bmatrix} 0 \\ 0 \\ v_x b_1 \end{bmatrix} \mathbf{u}.$$

The performance output \mathbf{z} can be rewritten in the form

$$\mathbf{z} = F_p \mathbf{x}_p + G_p \mathbf{u} \quad (6)$$

where

$$F_p = \mathcal{W} \begin{bmatrix} 0 & 0 & 1 & 0 \\ 0 & 0 & 0 & 1 \\ v_x a_{11} & v_x a_{12} & 0 & 0 \end{bmatrix}, \quad G_p = \mathcal{W} \begin{bmatrix} 0 \\ 0 \\ \frac{2C_f}{M} \end{bmatrix}.$$

C. Standard Model for \mathcal{H}_2 Path Following Control

From the definitions of the vehicle model Σ_p in (4), the road model Σ_w in (5) and the performance vector \mathbf{z} in (6), the standard model $\Sigma(v_x)$ ¹ is easily constructed as

$$\Sigma(v_x) : \begin{cases} \dot{\mathbf{x}} = A(v_x)\mathbf{x} + B(v_x)\mathbf{u} + E(v_x)\mathbf{w} \\ \mathbf{z} = F(v_x)\mathbf{x} + G\mathbf{u}, \quad \mathbf{y} = C\mathbf{x} \end{cases} \quad (7)$$

¹The notation $\Sigma(v_x)$ is used to clarify that the system dynamics depends explicitly on the time-varying speed v_x .

where $\mathbf{x}^\top = [\mathbf{x}_p^\top \quad \mathbf{x}_w^\top]$, $\mathbf{y}^\top = [\mathbf{y}_p^\top \quad \mathbf{y}_w^\top]$, $\mathbf{w}^\top = [f_w \quad \delta_w]$

$$A(v_x) = \begin{bmatrix} A_p & E_{p2} \\ 0 & A_w \end{bmatrix}, \quad B(v_x) = \begin{bmatrix} B_p \\ 0 \end{bmatrix}, \quad F(v_x)^\top = \begin{bmatrix} F_p^\top \\ 0 \end{bmatrix}, \\ E(v_x) = \text{diag}(E_{p1}, B_w), \quad C = \text{diag}(C_p, C_w), \quad G = G_p.$$

Note that the premise variables of (7), *i.e.*, v_x , $\frac{1}{v_x}$, $\frac{1}{v_x^2}$, are functions of the vehicle speed which is measured and bounded

$$v_{\min} \leq v_x \leq v_{\max}, \quad v_{\min} = 5 \text{ [m/s]}, \quad v_{\max} = 30 \text{ [m/s]}. \quad (8)$$

Besides the bounds on the vehicle speed given in (8), those of the vehicle acceleration are also given

$$a_{\min} \leq a_x = \dot{v}_x \leq a_{\max}, \quad a_{\max} = -a_{\min} = 4 \text{ [m/s}^2\text{]}. \quad (9)$$

The above *physical* bounds on the longitudinal acceleration represents the limitation of the theoretical kinematic centripetal acceleration of the vehicle [31]. As shown later, a judicious consideration of the bounds given in (8) and (9) in the control design allows reducing the design conservatism.

IV. FUZZY STATIC OUTPUT FEEDBACK CONTROL DESIGN WITH \mathcal{D} -STABILITY CONCEPT

To avoid using costly vehicle sensors while keeping a simple control structure, we present hereafter an LMI-based solution to design \mathcal{H}_2 SOF controllers for T-S fuzzy systems. The concept of \mathcal{D} -stability is exploited to improve the transient performance. The proposed theoretical results are then applied to the path following control of autonomous vehicles.

A. Problem Definition and Preliminaries

For generality, consider a T-S fuzzy system as follows [32]:

$$\Sigma(\theta) : \begin{cases} \dot{\mathbf{x}} = \sum_{i=1}^N \eta_i(\theta) (A_i \mathbf{x} + B_i \mathbf{u} + E_i \mathbf{w}) \\ \mathbf{z} = \sum_{i=1}^N \eta_i(\theta) (F_i \mathbf{x} + G_i \mathbf{u}), \quad \mathbf{y} = \sum_{i=1}^N \eta_i(\theta) C_i \mathbf{x} \end{cases} \quad (10)$$

where $\mathbf{x} \in \mathbb{R}^{n_x}$ is the state, $\mathbf{u} \in \mathbb{R}^{n_u}$ is the control input, $\mathbf{w} \in \mathbb{R}^{n_w}$ is the disturbance, $\mathbf{z} \in \mathbb{R}^{n_z}$ is the controlled output, and \mathbf{y} is the measured output. It is assumed that the premise variable $\theta(t) = [\theta_1(t) \dots \theta_p(t)]^\top$ and its rate of variation $\dot{\theta}(t)$ are smooth and respectively valued in the hypercubes

$$\Theta = \{(\theta_1, \dots, \theta_p)^\top : \theta_j \in [\underline{\theta}_j, \bar{\theta}_j], j \in \Omega_p\}, \\ \Theta_d = \{(\dot{\theta}_1, \dots, \dot{\theta}_p)^\top : \dot{\theta}_j \in [\underline{v}_j, \bar{v}_j], j \in \Omega_p\},$$

where $\underline{\theta}_j \leq \bar{\theta}_j$ (respectively $\underline{v}_j \leq \bar{v}_j$) are *known* bounds on θ_j (respectively $\dot{\theta}_j$), for $j \in \Omega_p$. For conciseness, let us denote $\Pi(\theta) = \sum_{i=1}^N \eta_i(\theta) \Pi_i$, with $\Pi_i \in \{A_i, B_i, E_i, F_i, G_i, C_i\}$, $i \in \Omega_N$. Assume also that the time-varying matrices $\Pi(\theta)$ of (10), with $\Pi \in \{A, B, E, F, G, C\}$, are continuous on the hypercube Θ . The membership functions (MFs) $\eta_i(\theta)$ are continuously differentiable and belong to the simplex

$$\Delta_\theta = \left\{ \eta(\theta) \in \mathbb{R}^N : \sum_{i=1}^N \eta_i(\theta) = 1, \eta_i(\theta) \geq 0, \forall \theta \in \Theta \right\}.$$

Since $(\theta, \dot{\theta}) \in \Theta \times \Theta_d$, the lower bound ϕ_{i1} and the upper bound ϕ_{i2} of $\eta_i(\theta)$ can be easily obtained as follows:

$$\eta_i(\theta) \in [\phi_{i1}, \phi_{i2}], \quad \phi_{i1} \leq \phi_{i2}, \quad i \in \Omega_N. \quad (11)$$

Consider the following fuzzy SOF controller:

$$\mathbf{u} = \sum_{i=1}^N \eta_i(\theta) K_i \mathbf{y} = K(\theta) \mathbf{y}. \quad (12)$$

From (10) and (12), the closed-loop system is represented as

$$\Sigma_{cl}(\theta) : \begin{cases} \dot{\mathbf{x}} = \hat{A}(\theta) \mathbf{x} + E(\theta) \mathbf{w} \\ \mathbf{z} = \hat{F}(\theta) \mathbf{x}, \quad \mathbf{y} = C(\theta) \mathbf{x} \end{cases} \quad (13)$$

where

$$\begin{aligned} \hat{A}(\theta) &= A(\theta) + B(\theta)K(\theta)C(\theta), \\ \hat{F}(\theta) &= F(\theta) + G(\theta)K(\theta)C(\theta). \end{aligned}$$

For engineering applications, the transient behaviors of the closed-loop systems should be studied since guaranteeing only the stability property is not sufficient for practical performance. Here, desirable time response and closed-loop damping are enforced for path following control via \mathcal{D} -stability concept. To this end, LMI regions are defined as follows.

Definition 1 (LMI Regions). A subset \mathcal{D} of the complex plane \mathbb{C} is called an LMI region if there exist a symmetric matrix $\mathbf{X} \in \mathbb{R}^{m \times m}$ and a matrix $\mathbf{Y} \in \mathbb{R}^{m \times m}$ such that

$$\mathcal{D} = \{z \in \mathbb{C} : f_{\mathcal{D}}(z) \prec 0\},$$

with $f_{\mathcal{D}}(z) = \mathbf{X} + z\mathbf{Y} + \bar{z}\mathbf{Y}^{\top}$ and \bar{z} is the complex conjugate of z . Note that the characteristic function $f_{\mathcal{D}}(z)$ takes values in the space of $m \times m$ Hermitian matrices. Some useful LMI regions in control applications include, e.g., α -stability regions, vertical strips, disks, conic sectors [25]. The following lemma guarantees the \mathcal{D} -stability of a matrix \mathbf{A} , i.e., all the eigenvalues of \mathbf{A} are located inside the region \mathcal{D} , see [25].

Lemma 1. A matrix \mathbf{A} is \mathcal{D} -stable if and only if there exists a symmetric matrix \mathbf{P} such that

$$\mathbf{X} \otimes \mathbf{P} + \text{He}(\mathbf{Y} \otimes \mathbf{A}\mathbf{P}) \prec 0, \quad \mathbf{P} \succ 0.$$

As an example, the disk $\mathcal{D}(\alpha, \mathbf{r})$ of radius \mathbf{r} and center $(-\alpha, 0)$ is an LMI region with the following characteristic function:

$$f_{\mathcal{D}}(z) = \begin{bmatrix} -\mathbf{r} & \alpha + z \\ \alpha + \bar{z} & -\mathbf{r} \end{bmatrix}. \quad (14)$$

The associated \mathcal{D} -stability of \mathbf{A} is guaranteed if and only if

$$\begin{bmatrix} -\mathbf{r}\mathbf{P} & \alpha\mathbf{P} + \mathbf{A}^{\top}\mathbf{P} \\ \alpha\mathbf{P} + \mathbf{P}\mathbf{A} & -\mathbf{r}\mathbf{P} \end{bmatrix} \prec 0, \quad \mathbf{P} \succ 0. \quad (15)$$

This paper proposes an LMI-based algorithm to deal with the following control problem.

Problem 1. Given a T-S fuzzy system $\Sigma(\theta)$ as in (10) with $\theta(t) \in \Theta$, $\forall t > 0$. Determine the control gains K_i , for $i \in \Omega_N$, such that the SOF controller (12) stabilizes $\Sigma(\theta)$ while

- minimizing the upper bound of the \mathcal{H}_2 -norm $\|\Sigma_{cl}(\theta)\|_2$, specified later, for disturbance attenuation purposes, and
- guaranteeing a desirable transient response of (13) which is predefined through an appropriate LMI region.

For control design, the following parameter-dependent Lyapunov function (PDLF) candidate is considered:

$$\mathbb{V}(\mathbf{x}) = \mathbf{x}^{\top} \left(\sum_{i=1}^N \eta_i(\theta) Q_i \right)^{-1} \mathbf{x} = \mathbf{x}^{\top} Q(\theta)^{-1} \mathbf{x} \quad (16)$$

where $Q_i \succ 0$, for $\forall i \in \Omega_N$. The following result on \mathcal{H}_2 control can be found in [31].

Lemma 2. Consider system $\Sigma_{cl}(\theta)$ defined in (13) with $\theta(t) \in \Theta$, $\forall t > 0$. If there exist a symmetric parameter-dependent matrix $Q(\theta) \in \mathbb{R}^{n_x \times n_x}$, a parameter-dependent matrix $Z(\theta) \in \mathbb{R}^{n_w \times n_w}$, and a scalar $\gamma > 0$ such that

$$\begin{bmatrix} \hat{A}(\theta)Q(\theta) + Q(\theta)\hat{A}(\theta)^{\top} - \dot{Q}(\theta) & \star \\ \hat{F}(\theta)Q(\theta) & -I \end{bmatrix} \prec 0 \quad (17)$$

$$\begin{bmatrix} Z(\theta) & \star \\ E(\theta) & Q(\theta) \end{bmatrix} \succ 0 \quad (18)$$

$$\text{trace}(Z(\theta)) < \gamma^2 \quad (19)$$

Then, the Lyapunov function (16) can be used to prove the stability of (13), and $\|\Sigma_{cl}(\theta)\|_2 < \gamma$ where the \mathcal{H}_2 -norm of the time-varying system $\Sigma_{cl}(\theta)$ is defined as follows [34]:

$$\|\Sigma_{cl}(\theta)\|_2^2 = \lim_{h \rightarrow \infty} \frac{1}{h} \int_0^h \text{trace} \left(\hat{F}(\theta(t))Q(\theta(t))\hat{F}(\theta(t))^{\top} \right) dt.$$

Note that \mathcal{H}_2 control is considered here to achieve a robust path following performance under the time-varying variation of the road curvature. Hence, this is especially interesting to improve the path following control during curve taking.

Remark 2. It is difficult to obtain an effective control solution from Lemma 2 for two reasons. First, the design conditions in Lemma 2 depend on both θ and its time-derivative $\dot{\theta}$. Second, condition (17) is expressed as a *nonlinear* matrix inequality. Based on this lemma, we will present a set of *tractable* conditions to design a fuzzy SOF controller (12).

B. LMI-Based Fuzzy Static Output Feedback Control Design

The following theorem provides conditions to design an SOF controller (12) for T-S fuzzy system (10). To ease the presentation, we assume that $C_i = C$, $\forall i \in \Omega_N$. The case with parameter-dependent output matrix is discussed afterwards.

Theorem 1. Given a T-S fuzzy system in (10) with $\theta(t) \in \Theta$, $\forall t > 0$. If there exist positive definite matrices $Q_i \in \mathbb{R}^{n_x \times n_x}$, matrices $M_i \in \mathbb{R}^{n_u \times n_y}$, $X \in \mathbb{R}^{n_y \times n_y}$, $Z_i \in \mathbb{R}^{n_w \times n_w}$, for $i \in \Omega_N$, and positive scalars γ , ϵ such that

$$\begin{bmatrix} Z_i & \star \\ E_i & Q_i \end{bmatrix} \succ 0 \quad (20)$$

$$\text{trace}(Z_i) < \gamma^2 \quad (21)$$

$$\Xi_{iiklm} \prec 0, \quad \Xi_{ijk lm} + \Xi_{jik lm} \prec 0 \quad (22)$$

for $i, j, k, l \in \Omega_N$, $m \in \Omega_2$, $i < j$ and $k \neq l$. Then, the SOF controller (12) stabilizes the T-S fuzzy system (10) and guarantees that $\|\Sigma(\theta)_{cl}\|_2 < \gamma$. Furthermore, the control feedback gains in (12) are computed as follows:

$$K_i = M_i X^{-1}, \quad i \in \Omega_N. \quad (23)$$

The quantity Ξ_{ijklm} in (22) is defined as

$$\Xi_{ijklm} = \text{He} \begin{bmatrix} \mathcal{X} & 0 & \epsilon B_i M_j \\ G_i M_j C + F_i Q_j & -I/2 & \epsilon G_i M_j \\ C Q_j - X C & 0 & -\epsilon X \end{bmatrix} \quad (24)$$

with $\mathcal{X} = A_i Q_j + B_i M_j C - \phi_{km}(Q_k - Q_l)/2$.

Proof. Multiplying (20) by $\eta_i(\theta) \geq 0$ and summing up for all $i \in \Omega_N$, we obtain (18). Similarly, (21) implies (19). Note that if (22) holds, then $X + X^\top \succ 0$. This guarantees the nonsingularity of X . Since $\eta(\theta) \in \Delta_\theta$, it follows that $\sum_{i=1}^N \dot{\eta}_i(\theta) = 0$. Then, we can easily deduce that

$$\dot{Q}(\theta) = \dot{\eta}_l(\theta) Q_l + \sum_{\substack{k=1 \\ k \neq l}}^N \dot{\eta}_k(\theta) Q_k = \sum_{\substack{k=1 \\ k \neq l}}^N \dot{\eta}_k(\theta) (Q_k - Q_l). \quad (25)$$

For any $\phi_{k1} \leq \dot{\eta}_k(\theta) \leq \phi_{k2}$ in (11), it follows that

$$\dot{\eta}_k(\theta) = \omega_{k1}(\theta) \phi_{k1} + \omega_{k2}(\theta) \phi_{k2}, \quad k \in \Omega_N \quad (26)$$

where $\omega_{k1}(\theta) = \frac{\phi_{k2} - \dot{\eta}_k(\theta)}{\phi_{k2} - \phi_{k1}}$ and $\omega_{k2}(\theta) = \frac{\dot{\eta}_k(\theta) - \phi_{k1}}{\phi_{k2} - \phi_{k1}}$. Clearly, $\omega_{kl}(\theta) \geq 0$ and $\sum_{l=1}^2 \omega_{kl}(\theta) = 1$. From (25) and (26), we get

$$\dot{Q}(\theta) = \sum_{\substack{k=1 \\ k \neq l}}^N \sum_{m=1}^2 \omega_{km}(\theta) \phi_{km} (Q_k - Q_l). \quad (27)$$

Using (24) and (27), inequality (22) implies that

$$\Upsilon_{ii}(\theta) \prec 0, \quad \Upsilon_{ij}(\theta) + \Upsilon_{ji}(\theta) \prec 0 \quad (28)$$

for $i, j \in \Omega_N$, $i < j$, where

$$\Upsilon_{ij}(\theta) = \text{He} \begin{bmatrix} \mathcal{Y}(\theta) & 0 & \epsilon B_i M_j \\ G_i M_j C + F_i Q_j & -I/2 & \epsilon G_i M_j \\ C Q_j - X C & 0 & -\epsilon X \end{bmatrix},$$

and $\mathcal{Y}(\theta) = A_i Q_j + B_i M_j C - \dot{Q}(\theta)/2$. Since $\eta_i(\theta) \geq 0$, $\forall i \in \Omega_N$, it follows from (28) that

$$\begin{aligned} & \sum_{i=1}^N \eta_i(\theta)^2 \Upsilon_{ii}(\theta) + \sum_{i=1}^N \sum_{i < j}^N \eta_i(\theta) \eta_j(\theta) (\Upsilon_{ij}(\theta) + \Upsilon_{ji}(\theta)) \\ &= \sum_{i=1}^N \sum_{j=1}^N \eta_i(\theta) \eta_j(\theta) \Upsilon_{ij}(\theta) \prec 0. \end{aligned} \quad (29)$$

Note that (29) can be rewritten in the form

$$\Phi(\theta) = \begin{bmatrix} \Phi_{11}(\theta) & \star & \star \\ \Phi_{21}(\theta) & -I & \star \\ \Phi_{31}(\theta) & \Phi_{32}(\theta) & -\epsilon(X + X^\top) \end{bmatrix} \prec 0 \quad (30)$$

where

$$\begin{aligned} \Phi_{11}(\theta) &= \text{He}(A(\theta)Q(\theta) + B(\theta)M(\theta)C) - \dot{Q}(\theta), \\ \Phi_{21}(\theta) &= G(\theta)M(\theta)C + F(\theta)Q(\theta), \\ \Phi_{31}(\theta) &= \epsilon M(\theta)^\top B(\theta)^\top + CQ(\theta) - XC, \\ \Phi_{32}(\theta) &= \epsilon M(\theta)^\top D_z(\theta)^\top. \end{aligned}$$

Multiplying (30) with

$$\mathcal{S} = \begin{bmatrix} I & 0 & B(\theta)M(\theta)X^{-1} \\ 0 & I & G(\theta)M(\theta)X^{-1} \end{bmatrix} \quad (31)$$

on the left and its transpose on the right yields (17) after simple manipulations. By Lemma 2, we can conclude the proof. \square

Remark 3. Using the PDLF (16), the information of θ and $\dot{\theta}$ is explicitly considered in the control procedure of Theorem 1 by exploiting the bounds ϕ_{kl} , $k \in \Omega_N$, $l \in \Omega_2$, in (11). This allows reducing the design conservatism. Indeed, if (22) is feasible with an arbitrarily high variation of the MFs, namely

$$\phi_{k1} \rightarrow -\infty, \quad \phi_{k2} \rightarrow +\infty, \quad \forall k \in \Omega_N.$$

Then, it is only possible that $Q_k \approx Q_l$, for $\forall k, l \in \Omega_N$, to minimize the effect of $\phi_{km}(Q_k - Q_l)$ involved in (24). Moreover, if $Q_i = Q$, for $\forall i \in \Omega_N$, in (16). Then, the common quadratic Lyapunov function $V(\mathbf{x}) = \mathbf{x}^\top Q^{-1} \mathbf{x}$ is straightforwardly recovered. This means that Theorem 1 includes precisely the quadratic design results.

Theorem 1 aims to design a stabilizing SOF controller (12) with a guaranteed \mathcal{H}_2 performance. To improve the transient response, it is desirable to take into account the LMI region $\mathfrak{D}(\alpha, \mathbf{r})$, described in Lemma 1, in the design procedure. The following theorem guarantees this \mathcal{D} -stability property.

Theorem 2. Consider the T-S fuzzy system $\Sigma_{cl}(\theta)$ in (13) with $\theta(t) \in \Theta$, $\forall t > 0$. All the eigenvalues of $\hat{A}(\theta)$ are within the LMI region $\mathfrak{D}(\alpha, \mathbf{r})$ if there exist positive definite matrices $\hat{Q}_i \in \mathbb{R}^{n_x \times n_x}$, matrices $M_i \in \mathbb{R}^{n_u \times n_y}$, $X \in \mathbb{R}^{n_y \times n_y}$, for $i \in \Omega_N$, and a positive scalar ϵ such that

$$\Gamma_{ii} \prec 0, \quad \Gamma_{ij} + \Gamma_{ji} \prec 0, \quad i, j \in \Omega_N, \quad i < j \quad (32)$$

where

$$\Gamma_{ij} = \begin{bmatrix} -\mathbf{r}\hat{Q}_j & \star & \star \\ \mathcal{Z}_{ij} & -\mathbf{r}\hat{Q}_j & \star \\ C\hat{Q}_j - XC & \epsilon M_j^\top B_i^\top & -\epsilon(X + X^\top) \end{bmatrix} \quad (33)$$

and $\mathcal{Z}_{ij} = \alpha\hat{Q}_j + A_i\hat{Q}_j + B_i M_j C$.

Proof. Since $\eta_i(\theta) \geq 0$, $\forall i \in \Omega_N$, it follows from (32) that

$$\begin{aligned} & \sum_{i=1}^N \eta_i(\theta)^2 \Gamma_{ii} + \sum_{i=1}^N \sum_{i < j}^N \eta_i(\theta) \eta_j(\theta) (\Gamma_{ij} + \Gamma_{ji}) \\ &= \sum_{i=1}^N \sum_{j=1}^N \eta_i(\theta) \eta_j(\theta) \Gamma_{ij} \prec 0. \end{aligned} \quad (34)$$

With Γ_{ij} defined in (33), inequality (34) can be rewritten as

$$\begin{bmatrix} -\mathbf{r}\hat{Q}(\theta) & \star & \star \\ \mathcal{Z}(\theta) & -\mathbf{r}\hat{Q}(\theta) & \star \\ C\hat{Q}(\theta) - XC & \epsilon M(\theta)^\top B(\theta)^\top & -\epsilon(X + X^\top) \end{bmatrix} \prec 0 \quad (35)$$

where $\mathcal{Z} = \alpha\hat{Q}(\theta) + A(\theta)\hat{Q}(\theta) + B(\theta)M(\theta)C$ and $\hat{Q}(\theta) = \sum_{i=1}^N \eta_i(\theta)\hat{Q}_i$. Multiplying (35) with

$$\mathcal{T} = \begin{bmatrix} I & 0 & 0 \\ 0 & I & B(\theta)M(\theta)X^{-1} \end{bmatrix} \quad (36)$$

on the left and its transpose on the right leads to

$$\begin{bmatrix} -\mathbf{r}\hat{Q}(\theta) & \star \\ [(\alpha + A(\theta) + B(\theta)K(\theta)C)\hat{Q}(\theta) & -\mathbf{r}\hat{Q}(\theta)] \end{bmatrix} \prec 0. \quad (37)$$

By a congruence transformation with $\text{diag}(\hat{Q}(\theta)^{-1}, \hat{Q}(\theta)^{-1})$, (37) is shown to be equivalent to (15) with $\mathbf{P} = \hat{Q}(\theta)^{-1}$ and $\mathbf{A} = \hat{A}(\theta)$. This concludes the proof. \square

The following result provides a solution for Problem 1.

Corollary 1. Given a T-S fuzzy system in (10) with $\theta(t) \in \Theta$, for $\forall t > 0$, and the LMI region $\mathfrak{D}(\alpha, \mathbf{r})$ with the characteristic function (14). If there exist positive definite matrices $Q_i \in \mathbb{R}^{n_x \times n_x}$, $\hat{Q}_i \in \mathbb{R}^{n_x \times n_x}$, matrices $M_i \in \mathbb{R}^{n_u \times n_y}$, $X \in \mathbb{R}^{n_y \times n_y}$, $Z_i \in \mathbb{R}^{n_w \times n_w}$, for $i \in \Omega_N$, and positive scalars γ, ϵ such that

$$\begin{aligned} \min_{\xi_i, i \in \Omega_N} \quad & \gamma^2 \\ \text{s.t.} \quad & (20), (21), (22) \text{ and } (32) \end{aligned} \quad (38)$$

where $\xi_i = (\epsilon, \gamma, Q_i, \hat{Q}_i, M_i, X, Z_i)$. Then, the SOF controller (12) with the control gains in (23) solves Problem 1.

Proof. This is a direct consequence of Theorems 1 and 2. \square

Remark 4. A similar reasoning can be adopted to generalize the result in Corollary 1 to cope with a parameter-dependent output matrix $C(\theta)$. This is accomplished by including the matrices C_i , $i \in \Omega_N$, accordingly in (22).

Remark 5. The extra variable X is introduced in the design conditions of Theorems 1 and 2 via congruence transformations with block-matrices \mathcal{S} and \mathcal{T} defined in (31) and (36). This special feature enables an LMI-based formulation with a single line search parameter for SOF control without requiring any matrix equality constraint and/or matrix rank condition as in most of existing works, see [4], [41] and related references. Such restrictive conditions are hardly tractable with available solvers, especially in T-S fuzzy control framework [23].

Remark 6. The design conditions in Corollary 1 are a set of LMIs with a line search over ϵ . The feedback gains K_i , $i \in \Omega_N$, can be easily computed with YALMIP toolbox [42]. The line search for ϵ was performed with 100 points linearly gridded over a logarithmic scale in $[10^{-5}, 10^5]$.

C. Application to Vehicle Path Following Control

1) *Vehicle fuzzy standard model:* The premise variable vector of system (7) is given as $\theta_* = \left[v_x \quad \frac{1}{v_x} \quad \frac{1}{v_x^2} \right]^\top$. Using the sector nonlinearity approach [32, Chapter 2], the T-S fuzzy representation (10) of the standard model (7) has $2^3 = 8$ linear subsystems. Such a representation leads to conservative results since v_x , $\frac{1}{v_x}$ and $\frac{1}{v_x^2}$ are considered *separately* even they are strongly dependent. To avoid this drawback while significantly reducing the design complexity for real-time implementation, the following variable change is used [30]:

$$v_x = \frac{v_0 v_1}{v_1 + v_0 \theta} \quad \Leftrightarrow \quad \frac{1}{v_x} = \frac{1}{v_0} + \frac{1}{v_1} \theta \quad (39)$$

where $v_0 = \frac{2v_{\min} v_{\max}}{v_{\min} + v_{\max}}$ and $v_1 = \frac{2v_{\min} v_{\max}}{v_{\min} - v_{\max}}$. The new premise variable θ satisfies

$$\theta_{\min} \leq \theta \leq \theta_{\max}, \quad \theta_{\min} = -1, \quad \theta_{\max} = 1. \quad (40)$$

Since $v_x = v_{\min}$ for $\theta = \theta_{\min}$ and $v_x = v_{\max}$ for $\theta = \theta_{\max}$, θ can be used to describe the variation of v_x between its lower and upper bounds. It is easily deduced from (39) that

$$\frac{a_{\min}}{a_0} \leq \dot{\theta} \leq \frac{a_{\max}}{a_0}, \quad a_0 = -\frac{v_0^2}{v_1}. \quad (41)$$

Moreover, applying Taylor's approximation as in [37] to the second expression of (39) leads to

$$v_x \simeq v_0 \left(1 - \frac{v_0}{v_1} \theta \right), \quad \frac{1}{v_x^2} \simeq \frac{1}{v_0^2} \left(1 + 2 \frac{v_0}{v_1} \theta \right). \quad (42)$$

Substituting expressions (39) and (42) into (7) leads to the following vehicle standard model:

$$\Sigma_v(\theta) : \begin{cases} \dot{\mathbf{x}} = A(\theta)\mathbf{x} + B(\theta)\mathbf{u} + E(\theta)\mathbf{w} \\ \mathbf{z} = F(\theta)\mathbf{x} + G\mathbf{u}, \quad \mathbf{y} = C\mathbf{x} \end{cases} \quad (43)$$

which is *linearly* dependent on θ . By the sector nonlinearity approach, $\Sigma_v(\theta)$ defined in (43) can be *exactly* represented in the T-S fuzzy form (10) where

$$\begin{aligned} \Lambda_1 &= \Lambda(\theta_{\min}), \quad C_1 = C_2 = C, \quad \eta_1(\theta) = (1 - \theta)/2, \\ \Lambda_2 &= \Lambda(\theta_{\max}), \quad G_1 = G_2 = G, \quad \eta_2(\theta) = (1 + \theta)/2, \end{aligned}$$

and $\Lambda \in \{A, B, E, F\}$.

Remark 7. The variable change (39) allows decreasing the number of parameter vertices from eight to two. This significantly reduces not only the design conservatism but also the numerical complexity of the control structure for real-time implementation. Moreover, given the bounds of θ and $\dot{\theta}$ in (40) and (41), it is straightforward to obtain

$$\phi_{11} \leq \dot{\eta}_1(\theta) \leq \phi_{12}, \quad \phi_{21} \leq \dot{\eta}_2(\theta) \leq \phi_{22},$$

where

$$\phi_{11} = \frac{-a_{\max}}{2a_0}, \quad \phi_{12} = \frac{-a_{\min}}{2a_0}, \quad \phi_{21} = \frac{a_{\min}}{2a_0}, \quad \phi_{22} = \frac{a_{\max}}{2a_0}.$$

2) *Theoretical illustrations:* By Corollary 1, the following control goals can be simultaneously achieved.

- The designed SOF controller stabilizes the vehicle system while minimizing the closed-loop \mathcal{H}_2 norm to guarantee a desirable path following under unknown road curvatures.
- Considering LMI region $\mathfrak{D}(1, 40)$ for control design, the corresponding decay rate and disk constraints enforce a settling time of about 1 [s] for the impulse response and to prevent fast controller dynamics, respectively.

Solving the optimization problem (38), the numerical solver takes 49.96 seconds to provide the following feedback gains:

$$\begin{aligned} K_1 &= [-0.0329 \quad -0.5097 \quad -0.0359 \quad 2.4492], \\ K_2 &= [-0.1072 \quad -0.3118 \quad -0.0348 \quad 3.4798]. \end{aligned}$$

Note that the feedback gains in (and also the Lyapunov matrices which are not given here for brevity) corresponding to two subsystems of the vehicle standard model (43) are significantly different. This also justifies *a posteriori* the interest of using the parameter-dependent controller (12) and the Lyapunov function (16) to improve the closed-loop performance.

Remark 8. The amplitudes of the feedforward gain entries corresponding to the road curvature ρ_r , *i.e.*, $K_{1\rho} = 2.4492$

and $K_{2\rho} = 3.4798$, are significantly important compared to other feedback entries. As highlighted in Section V, this represents the *prediction* capacity of the proposed \mathcal{H}_2 fuzzy SOF controller which is useful to improve the path following performance in case of tight curvatures, see also Remark 1.

We solve the optimization (38) for a fixed decay rate $\alpha = 1$ and different values of the radius r . As expected, the result in Fig. 3 shows that the minimal \mathcal{H}_2 upper bound γ of $\Sigma_v(\theta)$ decreases in function of r . Observe also that no feasible control solution can be found for this real-world application if $r < 26$. It is particularly interesting to note that for the same parameter data, the optimization (38) is *infeasible* for any values of decay rate α and radius r when imposing $Q_1 = Q_2$, *i.e.*, quadratic approach. This clearly demonstrates the advantage of exploiting the vehicle acceleration bounds via the PDLF (16) for the \mathcal{H}_2 T-S fuzzy control design, see Remark 3.

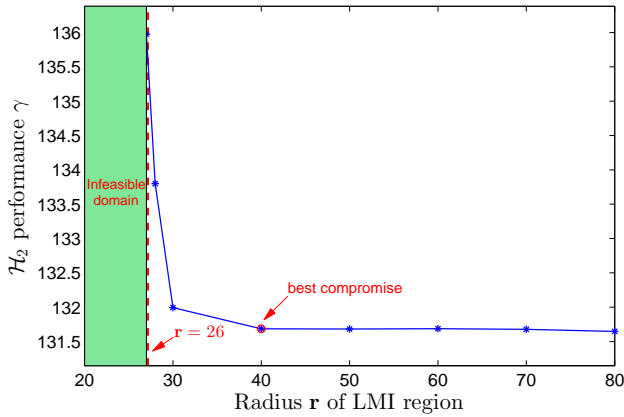


Fig. 3. Minimal \mathcal{H}_2 upper bound of $\Sigma_v(\theta)$ versus r of LMI region $\mathcal{D}(1, r)$.

V. EXPERIMENTAL RESULTS AND DISCUSSIONS

This section presents the experimental results to demonstrate the practical performance of the proposed path following control design. To this end, a series of hardware experiments is conducted under real-world driving situations with a SHERPA simulator. This interactive driving simulator is in the form of a Peugeot 206 vehicle fixed on a Stewart platform, see Fig. 4. The visual is displayed on a 240° wide panoramic screen. This dynamic simulator is structured around a SCANer network connecting fifteen PC-type workstations. All control algorithms were implemented in the SHERPA driving simulator through Matlab/Simulink software.

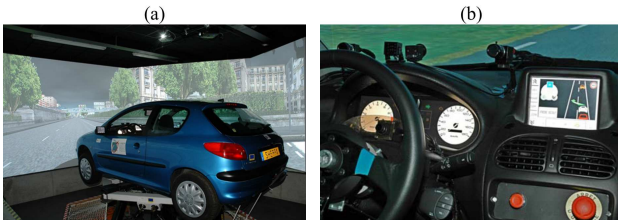


Fig. 4. (a) SHERPA driving simulator; (b) View of the simulator cockpit.

A. Experiment 1: Real-world Driving with Satory Test Track

This experiment aims to show the path following performance of the designed SOF controller obtained with the database of the Satory track, located 20 km west of Paris, France, see Fig. 5(a). As depicted in Fig. 5(b), this test track is composed of several curved sections including tight bends. The vehicle speed is highly *time-varying* and managed by a human driver during the whole test, see Fig. 5(c). For this real-world driving, observe in Figs. 5(d), (e), (f) and (g) that the proposed SOF controller provides a good path following performance with small tracking errors and a reasonable steering control angle even in cases of aggressive lateral accelerations (about 5 [m/s²]) when taking tight curves, see Fig. 5(h).

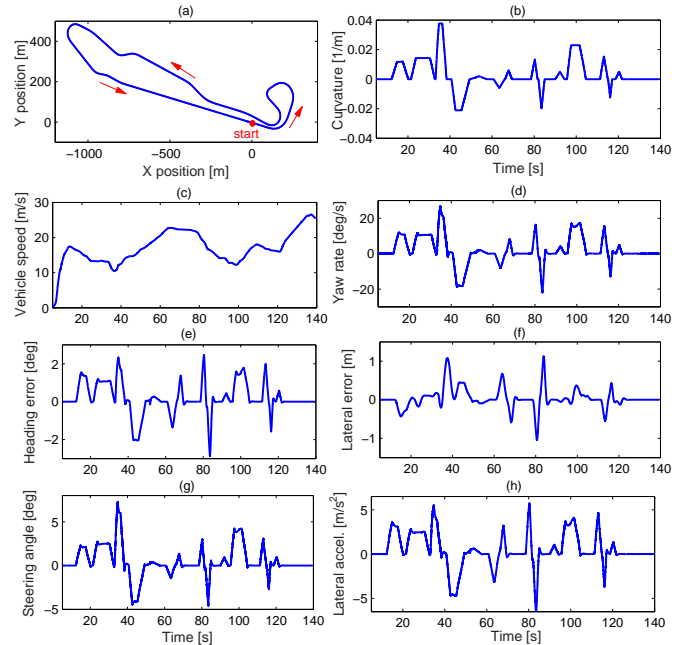


Fig. 5. Automatic path following performed with the Satory test track.

B. Experiment 2: Lane Change Maneuver

To verify the control performance under highly dynamic maneuvering, we assume that the autonomous vehicle must perform a lane change maneuver as illustrated in Fig. 6(a). This driving scenario leads to an important level of lateral acceleration as shown in Fig. 6(f). The vehicle responses obtained with the designed controller, corresponding to three vehicle speeds: $v_x = 30$ [km/h], $v_x = 40$ [km/h], and $v_x = 50$ [km/h], are shown in Fig. 6. Note that since the variation of the vehicle speed is explicitly taken into account in the \mathcal{H}_2 control design, a good path following performance is achieved with the proposed controller for three lane change tests. As expected, although the vehicle responses are quite similar under three different speeds, the tracking errors and the lateral acceleration increase when the vehicle speed becomes more important, see Figs. 6(b), (c), (d) and (f).

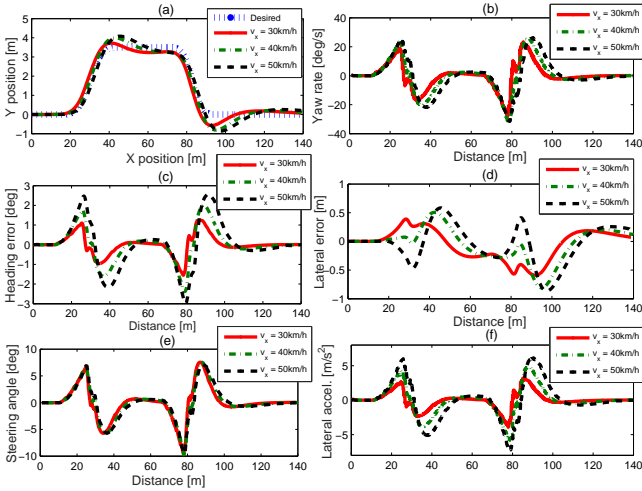


Fig. 6. Vehicle responses with respect to an obstacle avoidance maneuver at different vehicle speeds.

C. Experiment 3: Comparison of Path Following Performance

This test aims to show the interest of using the standard model (7) formalized in Section III for \mathcal{H}_2 control design. To this end, two following T-S fuzzy controllers are compared.

- **Controller 1:** This controller, designed in Section IV-C, is used in previous numerical/experimental experiments.
- **Controller 2:** The only difference of this controller compared to Controller 1 is that for its design, the road model (5) is not taken into account in the formulation of the standard model. Hence, Controller 2 does not have any prediction feature, see Remark 1.

To put in evidence the contribution of the feedforward control action of Controller 1, the two following cases are distinguished for the performance comparison.

1) *Case 1 (Comparison with a constant speed):* For this scenario, the vehicle must perform a path following task at a constant speed $v_x = 70$ [km/h] on a road section composed of small curvatures, see Figs. 7(a) and (b). Fig. 7 shows that a satisfactory performance is achieved with both SOF controllers. However, observe in Fig. 7(e) that the response of Controller 1 is faster than that of the pure feedback Controller 2. This allows Controller 1 to provide a better path following performance than Controller 2, especially in case of high road curvatures as depicted in Figs. 7(c) and (d). Fig. 7(f) represents the feedback-feedforward control partition of Controller 1. We can see that the feedforward action is always *in advance* compared to the feedback one, and proportional to the road curvature level. This clearly shows the *prediction* capacity of Controller 1 to improve the performance with curved trajectories, see Remark 8.

2) *Case 2 (Comparison with time-varying speed):* The vehicle performs now a driving task as in Case 1 with time-varying vehicle and more important road curvature, see Figs. 8(a) and (b), respectively. Similar to Case 1, Controller 1 provides also a better performance in this case as depicted in Fig. 8. In particular, for the last two curves with a road radius of 100 [m], Controller 2 cannot guarantee any more the path following task, and the vehicle goes out of the road, see

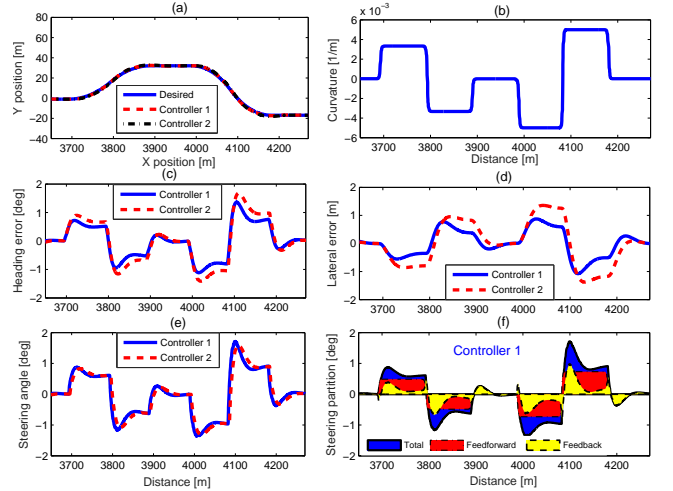


Fig. 7. Comparison of path following performance between two controllers in case of *constant* vehicle speed.

Figs. 8(c), (d), (e) and (f). This emphasizes the interest of the proposed \mathcal{H}_2 control design for path following of autonomous vehicles in various real-world driving conditions.

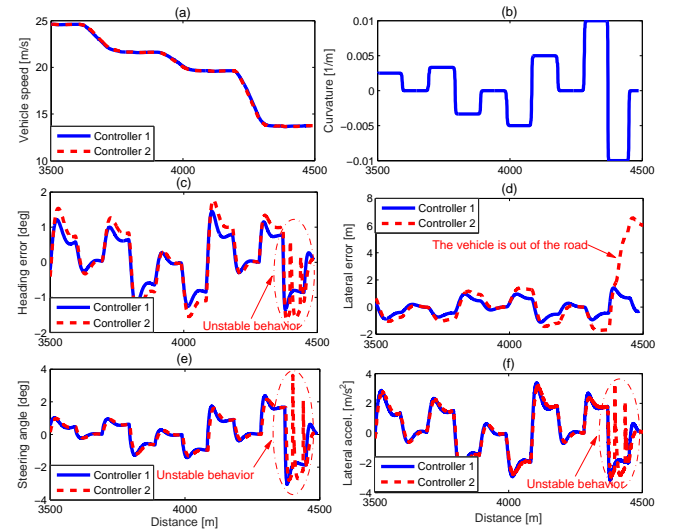


Fig. 8. Comparison of path following performance between two controllers in case of *time-varying* vehicle speed.

VI. CONCLUDING REMARKS

A new LMI-based method to design a path following controller for autonomous ground vehicles has been proposed. The \mathcal{H}_2 control design is formulated based on a conceptual standard vehicle model. To consider the time-varying nature of the vehicle speed, this standard model is transformed into a Takagi-Sugeno fuzzy system with a reduced level of numerical complexity. The proposed \mathcal{H}_2 SOF controller is of the simplest structure and only requires low-cost vehicle sensors for real-time implementation. In particular, the \mathcal{D} -stability concept is exploited to improve the closed-loop transient performance. Moreover, the physical bounds on the vehicle speed and acceleration are judiciously taken into account in

the \mathcal{H}_2 design via a parameter-dependent Lyapunov function to reduce the conservatism. The effectiveness of the new method is demonstrated through hardware experiments under various realistic driving conditions. In particular, the interest of the prediction feature of the proposed SOF controller is clearly put in evidence through appropriate comparisons with experimental results. Future works focus on the application of the proposed SOF control scheme to the driver-automation shared control issue [37].

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